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Polarimetry with Phased Array Antennas: Sensitivity and Polarimetric Performance Using Unpolarized Sources for Calibration

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Abstract—Polarimetric phased arrays require a calibration method that allows the system to measure the polarization state of the received signals. In this paper, we assess the polarimetric performance of two commonly used calibration methods that exploit unpolarized calibration sources. The first method obtains a polarimetrically calibrated beamforming solution from the two dominant eigenvectors of the measured signal covariance matrix. We demonstrate that this method is sensitivity equivalent to the theoretical optimal method, but suffers from an ambiguity that has to be resolved by additional measurements on (partially) polarized sources or by exploiting the intrinsic polarimetric quality of the antenna system. The easy-to-implement bi-scalar approach assumes that the feed system consists of two sets of orthogonally oriented antenna elements, each associated with one polarization. We assess its sensitivity and polarimetric performance over a wide field-of-view (FoV) using simulations of a phased array feed system for the Westerbork Synthesis Radio Telescope. Our results indicate that the sensitivity loss can be limited to 4.5% and that the polarimetric performance over the FoV is close to the best achievable performance. The latter implies that the intrinsic polarimetric quality of the antennas remains a crucial factor despite the development of novel polarimetric calibration methods.

Index Terms—phased array antennas, polarimetry, calibration, beamforming, far-field radiation pattern

I. INTRODUCTION

Polarimetric phased array antenna systems are commonly used in imaging radar applications [1], [2], but are relatively new in the field of radio astronomy. The radio astronomical community is developing the Square Kilometre Array (SKA) [3], a future radio telescope that is envisaged to be an order of magnitude more sensitive than present-day instruments. Phased array antennas will play a crucial role either as aperture array (AA) or as phased array feed (PAF) for reflector antennas. Several precursor and pathfinder systems using phased array antennas are currently in use or being developed. Examples of such instruments are the Low Frequency Array (LOFAR, AA) in Europe [4], the aperture tile-in-focus (APERTIF, PAF) upgrade of the Westerbork Synthesis Radio Telescope in The Netherlands [5], the Australian SKA Pathfinder (ASKAP, PAF) in the Western Australian Desert [6] and the Long Wavelength Array (LWA, AA) in the US [7].

The goals of these instruments for future radio astronomy research require high system sensitivity for detecting weak radio signals and accurate reconstruction of the polarization state of these signals. A polarimetric antenna system, capable of sampling the incident field by two orthogonally polarized receptors, can fully reconstruct the polarization state of the field. This reconstruction can be done by inverting a $2 \times 2$ transfer matrix that relates the two output signals of the receiver system to the polarization state of the field received by the system [8]. In polarimetric systems, calibration should not only compensate the gain differences between the receiving elements to provide maximum sensitivity at the beamformer outputs, but also ensure that the covariance between the two beamformer output signals allows proper reconstruction of the polarization state of the incident field. In a recent paper [9], the authors have developed a system model and used it to relate the astronomical performance criteria to standard IEEE definitions for polarimetric antennas and to find a beamforming algorithm that simultaneously optimizes for minimum system noise and polarimetric accuracy. In this paper, we use this framework to assess the polarimetric performance and sensitivity of two commonly used calibration methods that exploit unpolarized sources. This is particularly relevant, because the majority of extragalactic radio sources with a continuum spectrum, which are typically used for calibration of radio telescopes, are weakly polarized or unpolarized and hence calibration methods based on polarized reference sources are usually not applicable.

A recently proposed method exploits the two dominant eigenvectors of the signal covariance matrix measured on an unpolarized source with a dual-polarized array [10], which we will refer to as eigenvector method. This method may cause a large unknown change of the orientation of the polarization axes of the instrument, as we demonstrate in this paper, and is therefore unsuitable for application in actual systems without further polarimetric corrections. These polarimetric corrections either require additional measurements on polarized sources or relying on the intrinsic polarimetric quality of the system.

A second commonly used method exploits the fact that feed systems usually consist of two sets of orthogonally oriented antenna elements. For such systems, it is common...
practice to calibrate the two sets independently and to apply a single polarization correction at the end. This bi-scalar method imposes additional constraints on the system design, including manufacturing tolerances. We assess the stringency of these constraints by comparison with the theoretically optimal performance using theoretical analysis and simulations.

This paper is organized as follows. We start by introducing the system model and performance metrics used to assess the performance of the antenna system. In Sec. III we introduce the calibration methods and discuss their theoretical performance. We then introduce a simple analytic dipole model in Sec. IV to demonstrate the impact of the unitary ambiguity introduced when calibrating on an unpolarized source and show how the polarimetric quality of the methods exploiting the intrinsic polarimetric quality of the antenna system depends on the orthogonality between the feed systems. In Sec. V, we present simulations for an actual PAF system to assess the impact of using a bi-scalar instead of a full-polarimetric approach on the sensitivity and polarimetric performance over the field-of-view (FoV). We show that the sensitivity loss can be limited to 4.5% while the polarimetric performance over the FoV is comparable to the best achievable performance.

II. THEORY

A. System model

Figure 1 shows an $N$-element polarimetric phased array. The antenna system is assumed to be illuminated by a partially polarized source. The electric field intensity vector radiated by such a source is

$$\mathbf{E}(\mathbf{r}, t) = E_u(\mathbf{r}, t) \hat{u} + E_v(\mathbf{r}, t) \hat{v},$$

where $\hat{u}$ and $\hat{v}$ are orthogonal unit vectors according to a certain specific Ludwig’s definition [11] relative to the coordinate system of the array.

The antenna output signals are amplified to form the $N$-element output voltage vector $\mathbf{v}$ and are subsequently combined into the beamformer output voltages $v_1$ and $v_2$ using the $N \times 1$ beamformer weight vectors $\mathbf{w}_1$ and $\mathbf{w}_2$.

At a fixed position $\mathbf{r}$, $E_u(\mathbf{r}, t)$ and $E_v(\mathbf{r}, t)$ are complex random processes in the phasor or complex baseband representation. The polarization state of the field is determined by the correlation matrix of the two field components, which is

$$\mathbf{\Sigma} = \begin{bmatrix} \sigma_{uu} & \sigma_{uv} \\ \sigma_{vu} & \sigma_{vv} \end{bmatrix} = \begin{bmatrix} \langle |E_u|^2 \rangle & \langle E_u E_v^* \rangle \\ \langle E_u^* E_v \rangle & \langle |E_v|^2 \rangle \end{bmatrix},$$

where $\langle \cdot \rangle$ denotes the expected value. For an unpolarized source, we have $\mathbf{\Sigma} = \mathbf{I}$.

We will model the phased array antenna signal output in terms of the voltage response vectors of the array, $\mathbf{v}_u$ and $\mathbf{v}_v$, containing voltages at the array receiver outputs before beamforming induced by unit intensity, linearly polarized waves having their polarization aligned with $\hat{u}$ and $\hat{v}$ respectively. Theoretically, these voltages can be measured using a reference source producing two signals with perfectly orthogonal polarizations.

For an arbitrary polarized wave, the array signal voltage response vector can be formulated in terms of $\mathbf{v}_u$ and $\mathbf{v}_v$ as

$$\mathbf{v}_s = E_u \mathbf{v}_u + E_v \mathbf{v}_v.$$  (3)

The array output signal covariance matrix is

$$\mathbf{R}_s = \langle \mathbf{v}_s \mathbf{v}_s^H \rangle = \mathbf{V} \mathbf{\Sigma} \mathbf{V}^H,$$  (4)

where we have introduced $\mathbf{V} = [\mathbf{v}_u, \mathbf{v}_v]$. Assuming that the phased array system noise can be characterized by a noise covariance matrix $\mathbf{R}_n$, the covariance matrix of the array output voltage $\mathbf{v}$ can be described as

$$\mathbf{R} = \langle \mathbf{v} \mathbf{v}^H \rangle = \mathbf{R}_s + \mathbf{R}_n = \mathbf{V} \mathbf{\Sigma} \mathbf{V}^H + \mathbf{R}_n.$$  (5)

The noise covariance matrix can be determined using an off-source measurement on an empty part of the sky, i.e., a part of the sky without significant source structure. The noise covariance matrix includes factors such as noise coupling and spillover noise.

The beamformer output covariance matrix is obtained from the beamformer output voltages, $v_1 = \mathbf{w}_1^H \mathbf{v}$ and $v_2 = \mathbf{w}_2^H \mathbf{v}$, by

$$\mathbf{R}_o = \begin{bmatrix} v_1 & v_2 \end{bmatrix} \begin{bmatrix} v_1 & v_2 \end{bmatrix}^H = \begin{bmatrix} \langle |v_1|^2 \rangle & \langle v_1 v_2^* \rangle \\ \langle v_2^* v_1 \rangle & \langle |v_2|^2 \rangle \end{bmatrix}. $$  (6)

In terms of the signal and noise covariance matrices introduced earlier, this can be written as

$$\mathbf{R}_o = \begin{bmatrix} \mathbf{w}_1^H \mathbf{R} \mathbf{w}_1 & \mathbf{w}_1^H \mathbf{R} \mathbf{w}_2 \\ \mathbf{w}_2^H \mathbf{R} \mathbf{w}_1 & \mathbf{w}_2^H \mathbf{R} \mathbf{w}_2 \end{bmatrix} = [ \mathbf{w}_1 \mathbf{w}_2 ]^H \mathbf{R} [ \mathbf{w}_1 \mathbf{w}_2 ]$$

$$= \mathbf{W}^H (\mathbf{V} \mathbf{\Sigma} \mathbf{V}^H + \mathbf{R}_n) \mathbf{W}$$

$$= \mathbf{R}_{o,s} + \mathbf{R}_{o,n},$$  (7)

where $\mathbf{R}_{o,s}$ and $\mathbf{R}_{o,n}$ are the beamformer output covariance matrices due to the signal and the noise, respectively.
B. Useful concepts

1) Sensitivity equivalence: The combined sensitivity, expressed as the ratio of effective aperture area $A_e$ and system temperature $T_{sys}$ of the two beamformer outputs, the beam pair sensitivity, is determined by a linear combination of the two output signals. This can be obtained from [8]

$$\frac{A_e}{T_{sys}} = \frac{k_B B}{S_{sig} \text{SNR}} = \frac{k_B B}{S_{sig}} \frac{a^H W^H R_n W a}{a^H W^H R_n W a},$$

(8)

where $a = [a_1, a_2]^T$ is an arbitrary vector other than the null vector, $S_{sig}$ is the power flux density of the received signal expressed in W/m², $k_B$ is the Boltzmann constant and $B$ is the bandwidth.

As shown in [9], the beam pair sensitivity is bounded by

$$\frac{k_B B}{S_{sig} \lambda_{\min}} \leq \frac{A_e}{T_{sys}} \leq \frac{k_B B}{S_{sig} \lambda_{\max}},$$

(9)

where $\lambda_{\min}$ and $\lambda_{\max}$ are the smallest and largest eigenvalue of $C = V^H W (W^H R_n W)^{-1} W^H V$.

By replacing $W$ with $W' = WA$ where $A$ is an arbitrary invertible $2 \times 2$ matrix, it is easily seen that $C$ is independent of a linear transformation of the beam subspace and therefore of the polarimetric calibration. We will refer to beam pairs that are related by such a transformation as sensitivity equivalent beam pairs. This transformation signifies that all sensitivity equivalent beam pairs lie within the same two dimensional subspace of the $N$-dimensional space of complex valued $N$-element vectors. There are many possible rank two subspaces, but only one that includes the maximum sensitivity beamformer. Within each two dimensional subspace, there is one unique beam pair that is polarimetrically calibrated.

Transformations applied after beamforming necessarily stay within one two dimensional subspace. Sensitivity equivalence implies that the beamformer weights can be described as $WJ_{corr}$, where $J_{corr}$ is a $2 \times 2$ matrix describing a polarimetric correction. If a beamformer can be formulated in this form, the polarimetric correction can be done after beamforming without affecting the sensitivity bounds of the beamformer given by (9).

2) Jones matrices: In the noise free case or with noise estimated and subtracted, (7) reduces to

$$R_n = W^H V \Sigma V^H W = J \Sigma J^H,$$

(11)

where we have introduced the $2 \times 2$ Jones matrix $J = W^H V$. This Jones matrix represents the transfer function of the instrument including antennas, receiver chains and beamforming scheme, that transforms the two input voltages adhering to a suitable polarimetric definition into two output voltages, possibly adhering to another polarimetric definition. Figure 2 provides a system level view of the phased array antenna system. The polarimetric properties of the source are defined by the source covariance matrix $\Sigma$. This is transformed to the beamformer output covariance matrix $R_n$ (equal to $R_{sys}$ in the noise free case), that is used for further processing to produce a reconstructed source covariance matrix $\Sigma'$ that should ideally be proportional to $\Sigma$. An ideal system does not require polarimetric correction, since it has $J = I$, where $I$ denotes the identity matrix, i.e., it leaves the covariance matrix of the input signal unchanged and does not introduce so-called instrumental polarization. Since $J = W^H V$, the instrumental polarization introduced by the antennas and other analog electronics can be compensated for in the beamformer.

3) Max-SNR beamforming: The highest signal-to-noise ratio (SNR) for the $u$- and $v$-polarized signal is achieved by the max-SNR beamformer [12]

$$W_{SNR} = R_n^{-1} V.$$

(12)

Although this beamformer does not calibrate the polarimetric response of the array, it does provide the maximum sensitivity.

4) Optimal beamforming: If we know the voltage response vectors to two perfectly orthogonally polarized signals, $v_u$ and $v_v$, and the noise covariance matrix, $R_n$, we can derive optimal weights for the beamformer that ensures minimization of the noise in the measurement and perfect reconstruction of the polarimetric properties of the source. This optimization can be formulated as the constrained minimization problem

$$W_{opt} = \arg \min_W \text{tr} (W^H R_n W) \quad \text{subject to} \quad W^H V = I.$$

(13)

It can be shown that the solution to this optimization problem is given by [9]

$$W_{opt} = R_n^{-1} V (V^H R_n^{-1} V)^{-1}. $$

(14)

This pair of beamformer weight vectors minimizes the response to the system noise while constrained to be polarimetrically calibrated. We will refer to this calibration method as the optimal method. The factor $(V^H R_n^{-1} V)^{-1}$ can be interpreted as a Jones matrix that applies a polarimetric correction to the max-SNR beamformer weights. If the Jones matrix is invertible, an assumption that should hold for polarimetric arrays, the optimal beamformer is sensitivity equivalent to the max-SNR beamformer. Hence, the optimal and the max-SNR beamformer weights span the same subspace and within this subspace, the optimal beamformer picks the weight vectors that provide the optimal polarimetric response. The same response can be achieved with the max-SNR beamformer only with an additional polarimetric correction after beamforming.

5) XPD and XPI: Following standard IEEE definitions, the cross-polarization discrimination (XPD) and cross-polarization isolation (XPI) can be expressed in terms of Jones matrix elements as [13]

$$\begin{align*}
\text{XPD}_u &= \left| \frac{J_{11}}{J_{21}} \right|^2, \\
\text{XPI}_u &= \left| \frac{J_{11}}{J_{21}} \right|^2 \left| \frac{J_{22}}{J_{12}} \right|^2.
\end{align*}$$

(15a)
6) Intrinsic cross-polarization ratio: Since the goal of polarimetric phased arrays is to reconstruct the polarimetric properties of the source signal, preservation of these polarimetric properties by the Jones matrix $J$ of the instrument need not be a design goal by itself as long as the source coherency can be reconstructed by a polarimetric correction $J^{-1}$. This idea led to the definition of the intrinsic cross-polarization ratio (IXR). The IXR provides a measure for the reconstructability of $\Sigma$ (invertibility of $J$) and is defined as [13]

$$\text{IXR} = \frac{\kappa (J) + 1}{\kappa (J) - 1}^2,$$

where $\kappa (J)$ denotes the condition number of $J$.

The IXR provides an upper limit on the relative error in the reconstructed Stokes vector $S$ that is given by [13]

$$\frac{\| \Delta S_o \|}{\| S_o \|} \lesssim \left( 1 + \frac{4 \sqrt{\text{IXR}}}{1 + \text{IXR}} + \ldots \right) \left( \frac{\| \Delta M \|}{\| M \|} + \frac{\| \Delta S_o \|}{\| S_o \|} \right),$$

where $\| \cdot \|$ denotes the Euclidian norm, $\| \Delta M \|$ denotes the calibration error in the Mueller matrix and $\| \Delta S \|$ denotes the measurement error in the Stokes vector. Note that the term involving the IXR describes an increase of the relative Stokes error compared to a system with perfectly orthogonally polarized feeds. For example, if the noise on the observation causes a relative error (uncertainty) on the measured Stokes vector of 1% and the relative error in the instrument model (due to, e.g., calibration errors) is 1% as well, such a system would have about 1.4% relative error in the reconstructed Stokes vector. An IXR of 25 dB may (note that (17) gives an upper bound) cause a 22% increase in this error, which may therefore increase to 1.7%.

III. CALIBRATION USING AN UNPOLARIZED SOURCE

The majority of continuum extragalactic sources, which are typically used for calibration, are weakly polarized or unpolarized. Calibration of radio telescopes therefore requires methods that exploit unpolarized reference sources. In this section, we discuss three proposed methods. We will see that we cannot do a full polarimetric calibration of the system only using an unpolarized source. Two of the proposed methods rely on the intrinsic polarimetric characteristics of the instrument.

A. Eigenvector method

For a polarimetric array, neglecting estimation error, the signal covariance matrix $R_s$ measured on an unpolarized source has rank 2. If the system consists of two sets of orthogonally polarized feeds, there is hardly any correlation between the receiving elements in the two sets when measuring an unpolarized source. Intuitively, the two dominant eigenvectors will each be associated with one set of feeds. This naturally suggests the use of the two principal eigenvectors, $v_1$ and $v_2$, to form the maximum SNR eigenvector beamformer weight vectors [10]

$$W_{\text{eig}} = R_n^{-1}V_{\text{eig}},$$

where $V_{\text{eig}} = [v_1, v_2]$. We will refer to this approach as the eigenvector method.

To compare this beamformer with the optimal solution presented in the previous section, we note that the voltage response vectors $v_u$ and $v_v$ must span the same subspace as the eigenvectors $v_1$ and $v_2$. This implies that

$$V = V_{\text{eig}}J_{\text{eig}},$$

where the $2 \times 2$ Jones matrix $J_{\text{eig}}$ describes the transformation from $v_1$ and $v_2$ to $v_u$ and $v_v$. The weights obtained by the eigenvector method can thus be described as

$$W_{\text{eig}} = R_n^{-1}VJ_{\text{eig}}^{-1}.$$
system consists of two sets of feeds that have an orthogonal polarimetric response as proposed in [9]. For analysis of such a system, it is convenient to partition the signal covariance matrix as

$$R_s = \begin{bmatrix} R_{uu} & R_{uv} \\ R_{vu} & R_{vv} \end{bmatrix}. \quad (24)$$

The submatrices are $N/2 \times N/2$ matrices and we have assumed that the first $N/2$ elements are optimally matched to $\nu$-polarized signals while the second $N/2$ elements are optimally matched to $\nu$-polarized signals. The matrices

$$R_{u,u} = \begin{bmatrix} R_{uu} & 0 \\ 0 & 0 \end{bmatrix} \quad \text{and} \quad R_{v,v} = \begin{bmatrix} 0 & 0 \\ 0 & R_{vv} \end{bmatrix}, \quad (25)$$

have rank one with principal eigenvectors $\tilde{v}_u$ and $\tilde{v}_v$ respectively. These vectors can be used to find the approximate Jones matrix

$$\tilde{J} = W_e^{H} \tilde{V}, \quad (26)$$

where $\tilde{V} = [\tilde{v}_u, \tilde{v}_v]$. This Jones matrix can be used to calibrate the beam pair to obtain

$$W_{\text{approx}} = W_e^{\text{eig}} \tilde{J}^{-H}. \quad (27)$$

Since $\tilde{v}_u$ and $\tilde{v}_v$ are only determined up to a scale factor, further normalization may be required as discussed in [9].

C. Bi-scalar method

Most astronomical phased array systems consist of two sets of feeds, each optimally matched to a single polarization. This can be exploited by calibrating and beamforming both feed sets separately, which simplifies the design of the system considerably, since this approach requires two identical processing systems that each have to deal with only $N/2$ signals, instead of a single system with $N$ inputs, thereby simplifying signal routing and saving half the compute power for correlation of the input signals. This is referred to as a bi-scalar approach. Since this method treats both sets separately, it ignores the cross-terms between the two sets of elements in the signal and noise covariance matrices. For our analysis, it is therefore convenient to partition these matrices as indicated in (24). We can then formulate the bi-scalar beamformer as

$$W_{\text{bi-s}} = \begin{bmatrix} R_{uu}^{-1} & 0 \\ 0 & R_{vv}^{-1} \end{bmatrix} [\tilde{v}_u, \tilde{v}_v]. \quad (28)$$

If the two feed sets are perfectly matched to $\nu$- and $\nu$-polarized signals respectively such that $R_{uv} = R_{vu} = 0$, the bi-scalar approach gives the same result as the optimal method or the eigenvector method and is therefore sensitivity equivalent. Otherwise, the bi-scalar beamformer introduces a beamforming error due to neglecting the cross-polarization response of the elements. The impact on sensitivity depends on the antenna responses. Using (9) we can determine the loss in sensitivity for a specific antenna system.

A full polarimetric beamformer combines the $\nu$-polarized power picked up as co-polarization in the $\nu$-elements and as cross-polarization of the $\nu$-elements. The latter contribution is ignored by a bi-scalar beamformer. To get a feel for the implications of ignoring this term, we note that, in general, the voltage output of the beamformer is given by

$$W^{H}v = \begin{bmatrix} w_{u,u}^{H} & w_{u,v}^{H} \\ w_{v,u}^{H} & w_{v,v}^{H} \end{bmatrix} v$$

$$= \left( \begin{bmatrix} w_{u,u}^{H} & 0 \\ 0 & w_{v,v}^{H} \end{bmatrix} + \begin{bmatrix} 0 & w_{u,v}^{H} \\ 0 & 0 \end{bmatrix} \right) v, \quad (29)$$

where $w_{u,v}$ denotes the weight vector assigned to the $\nu$-polarized elements for the beamformer output associated with $\nu$-polarized signals and similar definitions for $w_{u,u}$, $w_{v,u}$ and $w_{v,v}$.

Since the weights $w_{u,v}$ need to be applied to the $\nu$-polarized elements although they are associated with $\nu$-polarized signals, we can exploit the ability of typical PAF systems to form a cross-polarization beam for the signals from the $\nu$-polarized elements and similarly for the $\nu$-polarized elements [16]. Once both co- and cross-polarized beams are formed, we can add the appropriate beam signals to reconstruct the output signals of a full polarimetric beamformer. This approach doubles the number of beams to be formed. Since the total bandwidth of the beamformer (number of beams times the bandwidth per beam) is limited by the digital hardware, we can only apply this scheme by sacrificing half the bandwidth per beam to allow for twice as many beams (the co- and cross-polarized beams). This reduces the sensitivity for continuum sources by a factor $\sqrt{2}$ and the survey speed by a factor 2. This may not seem attractive, but some observations, such as interferometric observations with other telescope systems, may not need the full bandwidth of the system in which case this scheme may be applied without its drawbacks. This is an important conclusion for instruments with a bi-scalar design that can form multiple beams within the FoV like APERTIF. However, calculation of these weights requires knowledge of the full signal and noise covariance matrices, which implies that these systems still need to provide a facility that can correlate the signals from any feed pair in the system for calibration of the array, although, for example, with a reduced bandwidth.

IV. DIPOLAR MODEL ANALYSIS

In this section, we present a simple dipole model and use it to provide some insight in the impact of the unitary ambiguity discussed in the previous section on the polarimetric performance of the instrument. We also use this dipole model to assess the impact of non-orthogonality in the polarimetric response of the receiving elements for the methods that rely on the intrinsic orthogonality of the feed sets.

A. Description of the dipole model

For this simple model, we assume that each antenna consists of two co-located ideal dipoles in the $(x, y)$-plane making an angle $\phi$ with each other. The open circuit responses of the dipoles for broadside incidence are then proportional to

$$V_{\text{oc}} \propto \begin{bmatrix} 1 \\ \gamma \cos \phi \\ \gamma \sin \phi \end{bmatrix}, \quad (30)$$
Since we are interested in the impact of non-orthogonality, the eigenvectors of the signal covariance matrix given by (31).

B. Eigenvalue decomposition

Numerical model.

Differences are primarily due to the finite strip width of the circuit voltages obtained from the EM-simulation with those especially for the crucial range where $\phi$. These results show that our analytical model is rather accurate, $\Delta$. Figure 3 compares the open circuited case, i.e., to assume that the antenna elements distance $\lambda/2$ and inter-element distance $\Delta z = 2 w$. Figure 3 compares the open circuit voltages obtained from the EM-simulation with those described by the analytical model while Fig. 4 makes a similar comparison for the elements of the noise covariance matrix. For convenience, we have assumed $8kTR_{\text{rad}} = 1$ and $\gamma = 1$. These results show that our analytical model is rather accurate, especially for the crucial range where $\phi$ is close to $90^\circ$. The differences are primarily due to the finite strip width of the numerical model.

B. Eigenvalue decomposition

For the analysis of the eigenvector method, we compute the eigenvectors of the signal covariance matrix given by (31). Since we are interested in the impact of non-orthogonality between the dipoles, we assume that the dipoles have the same gain, i.e., that $\gamma = 1$. Solving for the eigenvalues using the characteristic polynomial, we find that

$$\lambda_{1,2} = 1 \pm \cos \phi.$$  (33)

We can now solve for the eigenvectors associated with each eigenvalue. It is straightforward to show that for $\phi \neq \pi/2 \mod \pi$,

$$V_{\text{eig}} = \frac{1}{2} \sqrt{2} \begin{bmatrix} 1 & 1 \\ 1 & -1 \end{bmatrix}$$  (34)

and that $V_{\text{eig}} = \mathbf{I}$ if $\phi = \pi/2 \mod \pi$. Although $V_{\text{eig}}$ shows a discontinuity at $\phi = \pi/2$, we will see that the response of the system remains continuous when using the eigenvector method. Although this analysis was done for a single antenna consisting of two crossed dipoles, it can easily be shown that the results also hold for an array of identical antennas where the coupling between antenna pairs is negligible. This implies that the results obtained from the analysis of a single antenna can also be applied to a full array.

C. Impact of the unitary ambiguity

In this section we will demonstrate the effect of the unitary ambiguity by comparing the Jones matrix and beamformer output signal covariance matrix for the optimal method and the eigenvector method. It is straightforward to show that for the optimal method

$$J_{\text{opt}} = W_{\text{opt}} V = \mathbf{I}$$  (35)

such that

$$R_{\text{o, a}} = J_{\text{opt}} J_{\text{opt}}^H = \mathbf{I}.$$  (36)

In a similar way, we can show that for the eigenvector method

$$J_{\text{eig}} = W_{\text{eig}} V = \frac{1}{\sqrt{2}} \begin{bmatrix} 1 & \frac{1 - \cos \phi}{\sin \phi} \\ 1 & -\frac{1 + \cos \phi}{\sin \phi} \end{bmatrix},$$  (37)

where we assumed a proportionality constant in (32) equal to unity. It is interesting to note that substituting $\phi = \pi/2$...
in (37) gives the same result as obtained for \( \mathbf{V}_{\text{eig}} = \mathbf{I} \)

i.e., the discontinuity at \( \phi = \pi/2 \mod \pi \) found in the
eigenvalue decomposition vanishes when the result is applied
in the eigenvector beamforming scheme. Using (37) we find
that the beamformer output signal covariance matrix for the
eigenvector method is given by

\[
R_{\text{o,s}} = \begin{bmatrix}
2 \sin^2(\phi/2) & 0 \\
0 & 2 \cos^2(\phi/2)
\end{bmatrix}.
\] (38)

Equation (37) shows that if \( \phi \) is close to \( 90^\circ \), i.e., if the
polarimetric responses of the dipoles are (almost) orthogonal,
the magnitudes of the entries of the Jones matrix are (almost)
equal. This indicates that the two input polarizations aligned
with \( \hat{u} \) and \( \hat{v} \) are mixed to form two output signals that
are aligned with two other axes. However, if we look at the
beamformer output signal covariance matrix for an unpolarized
source, it seems that the system preserves the properties of
the source. This counter intuitive result can be explained by
the unitary ambiguity, which works on the Jones matrix, but
cancels itself in the beamformer output signal covariance ma-
trix, i.e., we have developed a beamforming scheme that gives
perfect results for unpolarized sources, but gives erroneous
results in observations on polarized sources.

It will also yield wrong results if the two beamformer output
signals are correlated to the two beamformer output signals
of another antenna system with a well-defined polarization.
This situation may occur in practice when multiple telescope
systems are linked together. Hence, it is important that the
voltage response of the system described by the Jones matrix is
well defined. This argument shows that the eigenvector method
is not suitable for use in an actual system unless appropriate
corrections are made to the beamformer output signals.

If we apply the bi-scalar approximate calibration discussed
in Sec. III-B to the dipole model, we find

\[
\mathbf{J}_{\text{approx}} = \mathbf{W}_{\text{approx}}^H \mathbf{V} = \begin{bmatrix}
1 & 0 \\
\cos \phi & 1
\end{bmatrix}.
\] (39)

This shows that if the dipoles are close to orthogonal, i.e.,
if \( \phi \approx 90^\circ \), then \( \mathbf{J}_{\text{approx}} \approx \mathbf{I} \), which is close to the
desired response. This shows that the unitary ambiguity can
be resolved by the intrinsic properties of the system, but that
the accuracy of that correction depends on the orthogonality
in the polarimetric response of the two feeds.

D. Impact of non-orthogonality

In our next simulation, we look at the impact of non-
orthogonality between the dipoles by comparing the IXR as
defined in (16) of the beamformers for different inter-dipole
angles. Since \( \mathbf{J} \propto \mathbf{I} \) for the optimal method, the IXR is infinite
for this method regardless of the orientation of the dipoles.
The IXR for the optimal method is therefore not shown in
Fig. 5. As derived in the appendix, the IXR for the eigenvector
method is conveniently described by

\[
\text{IXR}_{\text{eig}} = \frac{1}{\left( 1 + \tan(\phi/2) \right)^2}.
\] (40)

Comparison of the IXR for the bi-scalar method and for the
eigenvector method with and without bi-scalar approximate
calibration shows that the eigenvector methods are not able
to produce a pair of beamformer output signals that is more
suitable for reconstruction of the polarimetric properties of the
input signal than the bi-scalar beamformer when the dipoles
are close to orthogonal. This indicates, that these methods rely
on the polarimetric quality of the antenna system. An intuitive
explanation for this result, is that all these methods use an
unpolarized source for system calibration and thus have to
rely on the intrinsic polarization quality of the antenna system
to resolve the unitary ambiguity. Since most astronomical
 calibration sources are not or only weakly polarized, this
implies that a well-designed antenna system is invaluable, even
given the material presented in this paper. An IXR of 25 dB
limits the potential increase in the relative Stokes error during
reconstruction to 22% as indicated by (17), which requires
\( \phi \geq 83.7^\circ \).

Since the eigenvector method with bi-scalar correction is
sensitivity equivalent to the optimal beamformer and has the
same IXR as the bi-scalar beamformer, which has lower
sensitivity than the optimal method, it seems to be the best
method for calibration of a practical radio telescope system
on one of the available celestial calibration sources, which are
usually unpolarized.

It follows from (39) and the definitions given by (15a) and
(15b), that for the eigenvector method with bi-scalar correction

\[
\text{XPD}_u = \tan^2 \phi \quad \text{XPD}_v = \infty \quad \text{XPI}_u = \infty \quad \text{XPI}_v = \tan^2 \phi.
\]

Similarly, we find for the bi-scalar beamformer that

\[
\text{XPD}_u = \frac{1}{\cos^2 \phi \sin^2 \phi} \quad \text{XPD}_v = \infty \forall \phi \neq 0
\]

\[
\text{XPI}_u = \infty \quad \text{XPI}_v = \tan^2 \phi.
\]

These results are asymmetric in the two polarizations, since we
defined our dipole model such that one dipole is aligned with
one of the polarization axes. Since rotation of the polarization
axes is described by a unitary matrix, such a rotation does
not affect the condition number of the Jones matrix making the IXR insensitive to such a transformation. These results indicate that $\phi \geq 83.7^\circ$, required to achieve an IXR of 25 dB, corresponds to an XPD of at least 19 dB.

V. BI-SCALAR BEAMFORMER PERFORMANCE

The bi-scalar approach is commonly applied in actual phased array systems. However, in this paper, we have shown that the bi-scalar beamformer is not sensitivity equivalent to the optimal beamformer and that it relies on the intrinsic polarimetric orthogonality of the feed system. We would therefore like to assess the sensitivity and polarimetric performance of the bi-scalar beamformer in an actual system to see whether it provides acceptable performance. For this assessment, we use results from EM-simulations from the Aperture Tile-in-Focus (APERTIF) project. The goal of this project is to develop and build a PAF system for the Westerbork Synthesis Radio Telescope (WSRT) located in The Netherlands to increase its field-of-view (FoV) [5]. The APERTIF system will be able to produce 37 beams on the sky that will probably be arranged in a hexagonal pattern separated by about half power beam width as indicated in Fig. 6.

A. Performance in the compound beam centers

The APERTIF system was simulated using a full-wave EM package [18]. Figure 7 shows the average sensitivity of the two beamformer outputs for the optimal beamformer and the bi-scalar beamformer, while Fig. 8 shows the IXR of the bi-scalar beamformer. All results were obtained for the beam centers at 1.4 GHz. From these results, we conclude that use of a bi-scalar beamformer leads to about 4.5% sensitivity loss compared to the optimal beamformer and that the typical IXR will be about 38 dB with a peak value of 59 dB for the central compound beam. Note that the IXR in Fig. 8 is asymmetric with respect to the central beam with index 19. This is caused by the asymmetrical circular cavity terminating the tapered slot which has been bended sideways to reduce the length of the microstrip transmission line feeding the slot. Also, the antenna elements are positioned diagonally over a square ground plane which results in different element configurations per polarization at the corners of the array.

These results are similar to those found for an earlier APERTIF prototype system [16], [18]. Measurements done with the APERTIF prototype system mounted on one of the WSRT dishes confirmed the sensitivity loss, but also indicated that the practicalities of an actual system reduce the ratio of cross- to co-polarized power observed on an unpolarized source to about 28 dB [16]. This was considered acceptable, because the cross-polarization level can be improved by applying appropriate polarimetric corrections to the beamformer output signals while the sensitivity loss can be recovered by
forming cross- and co-polarized beams as discussed in Sec. III-C.

B. Behavior over FoV

In the previous subsection, we assessed the performance of the bi-scalar beamformer at the beam centers. Another concern is the behavior of the PAF voltage beams over their respective FoVs, since the image processing should correct for this response. Figure 9 therefore shows $|J_{12}|$ for the optimal method and the bi-scalar method over the FoV at 1.42 GHz. This shows that both beamformers suffer from the direction dependent polarimetric response of the two feed systems, but that the optimal beamformer does a better job at the beam centers of the compound beams towards the edges of the FoV. For the optimal beamformer, there is always a small region around the beam center in which the instrumental crosspolarization is less than -45 dB while the bi-scalar beamformer produces some beams with -30 dB crosspolarization in their field centers. This can be explained by the fact that the bi-scalar beamformer relies on the intrinsic polarimetric orthogonality between the two sets of orthogonally oriented antenna elements, which works very well in bore sight (the central beam), but deteriorates towards the edges of the FoV.

The results shown in Fig. 9 indicate that an appropriate correction for the polarimetric response of each PAF voltage beam is required in the image processing to reconstruct the polarimetric properties of the incident waves regardless of the beamforming approach used. The reconstructability of the polarization state of the received signals is measured by the IXR, which is shown in Fig. 10 for the bi-scalar beamformer. The simulations indicate that the inner 7 beams have an IXR better than 40 dB over almost their entire beam area, while the compound beams at the edges of the FoV still have an IXR of at least 25 dB. This gives an upper limit on the increase in the relative measurement error on the Stokes vector of 4% and 22% for the central beams and for the edges of the FoV respectively as predicted by (17). This should be sufficient to allow accurate reconstruction of polarized signals with limited sensitivity reduction due to image processing.

VI. CONCLUSIONS

In this paper we discussed the polarimetric and sensitivity performance of calibration schemes that exploit an unpolarized reference source. We demonstrated that the eigenvector method is sensitivity equivalent to the optimal beamformer. This implies that the eigenvector methods can exactly reproduce the result obtained from the optimal beamformer with an additional polarimetric correction after beamforming.

We have demonstrated that the eigenvector method is not suitable for use in an actual system without additional correction, because this method ignores the unitary ambiguity intrinsic to calibration on an unpolarized source. This ambiguity needs to be resolved either by imposing additional constraints on the system response, such as relying on the intrinsic polarimetric orthogonality between the feeds, or by additional calibration observation on two distinctly polarized sources.

The bi-scalar beamformer is not sensitivity equivalent to the optimal beamformer and relies on the intrinsic polarimetric
orthogonality of the feeds, but is easiest to implement in an actual system. We demonstrated that the bi-scalar beamformer can emulate the response of the optimal beamformer by forming cross- and co-polarized beams at the cost of halving the available beamforming bandwidth. We assessed the sensitivity loss and polarimetric performance of the bi-scalar beamformer using simulations for the APERTIF system, a PAF system currently being designed for the Westerbork Synthesis Radio Telescope. These simulations indicate that the sensitivity loss is about 4.5% while the typical IXR in the beam centers is about 38 dB. Since the bi-scalar beamformer relies on the polarimetric orthogonality of the feeds, the gradient of this orthogonality over the FoV causes variations in polarimetric response away from the beam centers that should be corrected for in the image processing. The simulations suggest that the IXR is at least 25 dB over the entire FoV, indicating that reconstruction of the polarimetric state of the incident wave should be possible with at most 22% increase in the relative error in the reconstructed image parameters. Since this is considered acceptable, our analysis indicates that XPD values as low as 20 dB inside the FoV are still acceptable, which is an important design requirement for future instruments like the SKA.

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APPENDIX

The condition number of a Jones matrix $J$ can be computed as

$$\kappa(J) = \frac{\sigma_{\text{max}}(J)}{\sigma_{\text{min}}(J)} = \left( \frac{\lambda_{\text{max}}(J^H J)}{\lambda_{\text{min}}(J^H J)} \right)^{1/2}, \tag{43}$$

where $\sigma(J)$ denotes the singular value of $J$ indicated by the subscript and $\lambda(J^H J)$ denotes the eigenvalue of $J^H J$ indicated by the subscript. Using $J_{\text{eig}}$ as given by (37) and solving for the characteristic polynomial, we find

$$\lambda_{\text{max}} = \cos^2 (\phi/2) \quad \text{and} \quad \lambda_{\text{min}} = \sin^2 (\phi/2), \tag{44}$$

such that

$$\kappa(J_{\text{eig}}) = \frac{\cos (\phi/2)}{\sin (\phi/2)}. \tag{45}$$

Substitution of this result in (16) and a little algebraic manipulation gives (40).

REFERENCES


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have led to the definition of APERTIF - a PAF system that is being developed at ASTRON to replace the current horn feeds in the Westerbork Synthesis Radio Telescope (WSRT). Dr. Ivashina was involved in the development of APERTIF during 2008-2010 and acted as an external reviewer at the Preliminary Design Review of the Australian SKA Pathfinder (ASKAP) in 2009. In 2002, she also stayed as a Visiting Scientist with the European Space Agency (ESA), ESTEC, in the Netherlands, where she studied multiple-beam array feeds for the satellite telecommunication system Large Deployable Antenna (LDA).

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